

## LMZ10501 1A SIMPLE SWITCHER® Nano Module with 5.5V Maximum Input Voltage

Check for Samples: [LMZ10501](#)

### FEATURES

- Integrated inductor
- Miniature form factor (3.0 mm x 2.5 mm x 1.425 mm)
- 8-pin LLP footprint
- -40°C to 125°C junction temperature range
- Adjustable output voltage
- 2.0MHz fixed PWM switching frequency
- Integrated compensation
- Soft start function
- Current limit protection

- Thermal shutdown protection
- Input voltage UVLO for power-up, power-down, and brown-out conditions
- Only 5 external components — resistor divider and 3 ceramic capacitors

### APPLICATIONS

- Point of load conversions from 3.3V and 5V rails
- Space constrained applications
- Low output noise applications

### DESCRIPTION

The LMZ10501 SIMPLE SWITCHER® nano module is an easy-to-use step-down DC-DC solution capable of driving up to 1A load in space-constrained applications. Only an input capacitor, an output capacitor, a small  $V_{CON}$  filter capacitor, and two resistors are required for basic operation. The nano module comes in 8-pin LLP footprint package with an integrated inductor. Internal current limit based softstart function, current overload protection, and thermal shutdown are also provided.

### Electrical Specifications

- Up to 1A output current
- Input voltage range 2.7V to 5.5V
- Output voltage range 0.6V to 3.6V
- Efficiency up to 95%

### Performance Benefits

- Small solution size
- Low output voltage ripple
- Easy component selection and simple PCB layout
- High efficiency reduces system heat generation



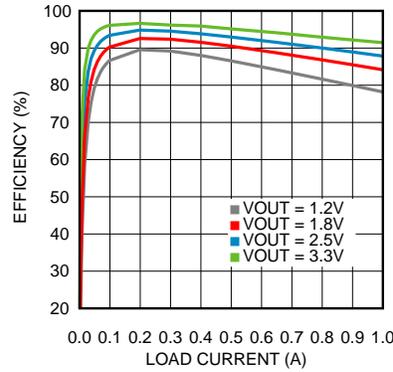
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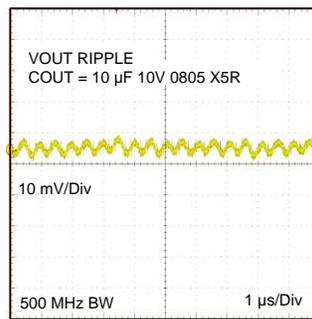
## System Performance

(Quick Overview Links: [V<sub>OUT</sub> = 1.2V](#), [1.8V](#), [2.5V](#), [3.3V](#))

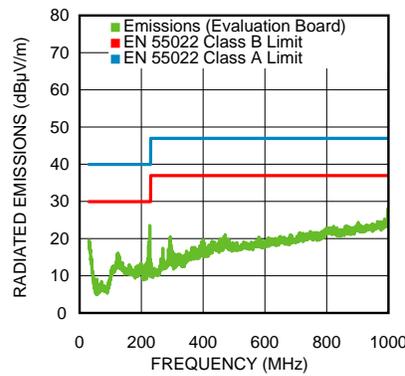
**Figure 1. Typical Efficiency at V<sub>IN</sub> = 3.6V**



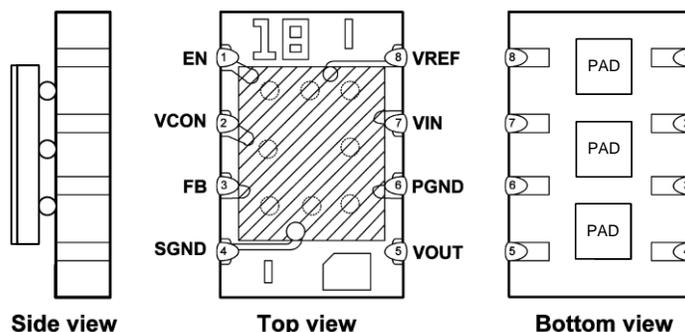
**Figure 2. Output Voltage Ripple**  
**V<sub>IN</sub> = 5.0V, V<sub>OUT</sub> = 1.8V, I<sub>OUT</sub> = 1A**



**Figure 3. Radiated EMI (CISPR22)**  
**V<sub>IN</sub> = 5.0V, V<sub>OUT</sub> = 1.8V, I<sub>OUT</sub> = 1A**



## Connection Diagram


**Figure 4.**
**Table 1. Pin Descriptions**

Pin #	Name	Description
1	EN	Enable Input. Set this digital input higher than 1.2V for normal operation. For shutdown, set low. Pin is internally pulled up to VIN and can be left floating for always-on operation.
2	VCON	Output voltage control pin. Connect to analog voltage from resistive divider or DAC/controller to set the VOUT voltage. $V_{OUT} = 2.5 \times V_{CON}$ . Connect a small (470pF) capacitor from this pin to SGND to provide noise filtering.
3	FB	Feedback of the error amplifier. Connect directly to output capacitor to sense $V_{OUT}$ .
4	SGND	Ground for analog and control circuitry. Connect to PGND at a single point.
5	VOUT	Output Voltage. Connected to one terminal of the integrated inductor. Connect output filter capacitor between VOUT and PGND.
6	PGND	Power ground for the power MOSFETs and gate-drive circuitry.
7	VIN	Voltage supply input. Connect ceramic capacitor between VIN and PGND as close as possible to these two pins. Typical capacitor values are between 4.7 $\mu$ F and 22 $\mu$ F.
8	VREF	2.35V voltage reference output. Typically connected to VCON pin through a resistive divider to set the output voltage.
	PAD	The 3 pads underneath the module are not internally connected to any node. These pads should be connected to the ground plane for improved thermal performance.



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

### Absolute Maximum Ratings <sup>(1)</sup>

VIN, VREF to SGND	-0.2V to +6.0V
PGND to SGND	-0.2V to +0.2V
EN, FB, VCON	(SGND -0.2V) to (VIN +0.2V) w/6.0V max
VOUT	(PGND -0.2V) to (VIN +0.2V) w/6.0V max
Junction Temperature ( $T_{J-MAX}$ )	+150°C
Storage Temperature Range	-65°C to +150°C
Maximum Lead Temperature	+260°C
ESD Susceptibility <sup>(2)</sup>	$\pm$ 2kV

- (1) Absolute Maximum Ratings are limits beyond which damage to the device may occur. Operating Ratings are conditions under which operation of the device is intended to be functional. For guaranteed specifications and test conditions, see the Electrical Characteristics.
- (2) The human body model is a 100pF capacitor discharged through a 1.5 k $\Omega$  resistor into each pin. Test method is per JESD-22-114.

**Operating Ratings** <sup>(1)</sup>

Input Voltage Range	2.7V to 5.5V
Recommended Load Current	0 mA to 1000 mA
Junction Temperature (T <sub>J</sub> ) Range	-40°C to +125°C

(1) Absolute Maximum Ratings are limits beyond which damage to the device may occur. Operating Ratings are conditions under which operation of the device is intended to be functional. For guaranteed specifications and test conditions, see the Electrical Characteristics.

**Thermal Properties**

Junction-to-Ambient Thermal Resistance ( $\theta_{JA}$ ), SEA08A Package <sup>(1)</sup>	120°C/W
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(1) Junction-to-ambient thermal resistance ( $\theta_{JA}$ ) is based on 4 layer board thermal measurements, performed under the conditions and guidelines set forth in the JEDEC standards JESD51-1 to JESD51-11.  $\theta_{JA}$  varies with PCB copper area, power dissipation, and airflow.

## Electrical Characteristics <sup>(1)</sup>

Specifications with standard typeface are for  $T_J = 25^\circ\text{C}$  only; Limits in **bold face** type apply over the operating junction temperature range  $T_J$  of  $-40^\circ\text{C}$  to  $125^\circ\text{C}$ . Minimum and maximum limits are guaranteed through test, design, or statistical correlation. Typical values represent the most likely parametric norm at  $T_J = 25^\circ\text{C}$ , and are provided for reference purposes only. Unless otherwise stated the following conditions apply:  $V_{IN} = 3.6\text{V}$ ,  $V_{EN} = 1.2\text{V}$ .

Symbol	Parameter	Conditions	Min (1)	Typ (2)	Max (1)	Units
<b>SYSTEM PARAMETERS</b>						
$V_{REF} \times \text{GAIN}$	Reference voltage x VCON to FB Gain	$V_{IN} = V_{EN} = 5.5\text{V}$ , $V_{CON} = 1.44\text{V}$	<b>5.7575</b>	5.875	<b>5.9925</b>	V
GAIN	VCON to FB Gain	$V_{IN} = 5.5\text{V}$ , $V_{CON} = 1.44\text{V}$	<b>2.4375</b>	2.5	<b>2.5750</b>	V/V
$V_{IN\_UVLO}$	VIN rising threshold			2.4		V
$V_{IN\_UVLO}$	VIN falling threshold			2.25		V
$I_{SHDN}$	Shutdown supply current	$V_{IN} = 3.6\text{V}$ , $V_{EN} = 0.5\text{V}$ (3)		11	<b>18</b>	$\mu\text{A}$
$I_q$	DC bias current into VIN	$V_{IN} = 5.5\text{V}$ , $V_{CON} = 1.6\text{V}$ , $I_{OUT} = 0\text{A}$		6.5	<b>8.5</b>	mA
$R_{DROPOUT}$	$V_{IN}$ to $V_{OUT}$ resistance	$I_{OUT} = 200\text{ mA}$		285	<b>425</b>	$\text{m}\Omega$
$I_{LIM}$	DC Output Current Limit	$V_{CON} = 0.24\text{V}$ (4)	<b>1125</b>	1350		mA
$F_{OSC}$	Internal oscillator frequency		1.75	2.0	2.25	MHz
$V_{IH\_ENABLE}$	Enable logic HIGH voltage		<b>1.2</b>			V
$V_{IL\_ENABLE}$	Enable logic LOW voltage				<b>0.5</b>	V
$T_{SD}$	Thermal shutdown	Rising Threshold		150		$^\circ\text{C}$
$T_{SD\_HYST}$	Thermal shutdown hysteresis			20		$^\circ\text{C}$
$D_{MAX}$	Maximum duty cycle			100		%
$T_{ON\_MIN}$	Minimum on-time			50		ns
$\theta_{JA}$	Package Thermal Resistance	20mm x 20mm board 2 layers, 2 oz copper, 0.5W, no airflow		118		$^\circ\text{C}/\text{W}$
		15mm x 15mm board 2 layers, 2 oz copper, 0.5W, no airflow		132		
		10mm x 10mm board 2 layers, 2 oz copper, 0.5W, no airflow		157		

(1) Min and Max limits are 100% production tested at  $25^\circ\text{C}$ . Limits over the operating temperature range are guaranteed through correlation using Statistical Quality Control (SQC) methods. Limits are used to calculate the Average Outgoing Quality Level (AOQL).

(2) Typical numbers are at  $25^\circ\text{C}$  and represent the most likely parametric norm.

(3) Shutdown current includes leakage current of the high side PFET.

(4) Current limit is built-in, fixed, and not adjustable.

## System Characteristics

The following specifications are guaranteed by design providing the component values in the Typical Application Circuit are used ( $C_{IN} = C_{OUT} = 10 \mu\text{F}$ , 6.3V, 0603, TDK C1608X5R0J106K). **These parameters are not guaranteed by production testing.** Unless otherwise stated the following conditions apply:  $T_A = 25^\circ\text{C}$ .

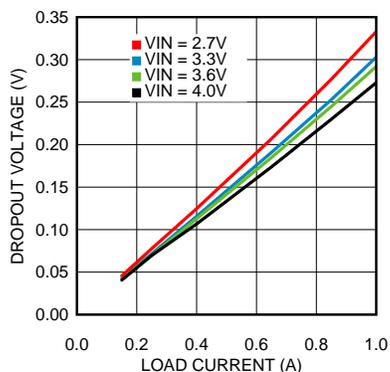
Symbol	Parameter	Conditions	Min	Typ	Max	Units
$\Delta V_{OUT}/V_{OUT}$	Output Voltage Regulation Over Line Voltage and Load Current	$V_{OUT} = 0.6\text{V}$ $\Delta V_{IN} = 2.7\text{V to } 4.2\text{V}$ $\Delta I_{OUT} = 0\text{A to } 1\text{A}$		$\pm 1.75$		%
$\Delta V_{OUT}/V_{OUT}$	Output Voltage Regulation Over Line Voltage and Load Current	$V_{OUT} = 1.5\text{V}$ $\Delta V_{IN} = 2.7\text{V to } 5.5\text{V}$ $\Delta I_{OUT} = 0\text{A to } 1\text{A}$		$\pm 0.92$		%
$\Delta V_{OUT}/V_{OUT}$	Output Voltage Regulation Over Line Voltage and Load Current	$V_{OUT} = 3.6\text{V}$ $\Delta V_{IN} = 4.0\text{V to } 5.5\text{V}$ $\Delta I_{OUT} = 0\text{A to } 1\text{A}$		$\pm 0.38$		%
VREF $T_{RISE}$	Rise time of reference voltage	EN = Low to High, $V_{IN} = 4.2\text{V}$ $V_{OUT} = 2.7\text{V}$ , $I_{OUT} = 1\text{A}$		10		$\mu\text{s}$
$\eta$	Peak Efficiency	$V_{IN} = 5.0\text{V}$ , $V_{OUT} = 3.3\text{V}$ $I_{OUT} = 200\text{ mA}$		95		%
	Full Load Efficiency	$V_{IN} = 5.0\text{V}$ , $V_{OUT} = 3.6\text{V}$ $I_{OUT} = 1000\text{ mA}$		91		
$V_{OUT}$ Ripple	Output voltage ripple	$V_{IN} = 5.0\text{V}$ , $V_{OUT} = 1.8\text{V}$ $I_{OUT} = 1000\text{ mA}$ <sup>(1)</sup>		10		mV pk-pk
Line Transient	Line transient response	$V_{IN} = 2.7\text{V to } 5.5\text{V}$ , $T_R = T_F = 10\ \mu\text{s}$ , $V_{OUT} = 1.8\text{V}$ , $I_{OUT} = 1000\text{mA}$		30		mV pk-pk
Load Transient	Load transient response	$V_{IN} = 5.0\text{V}$ $T_R = T_F = 40\ \mu\text{s}$ , $V_{OUT} = 1.8\text{V}$ $I_{OUT} = 100\text{mA to } 1000\text{ mA}$		30		mV pk-pk

(1) Ripple voltage should be measured across  $C_{OUT}$  on a well-designed PC board using the suggested capacitors.

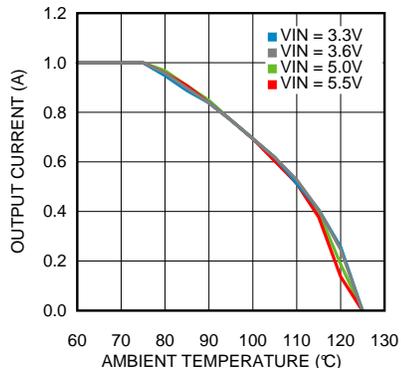
### Typical Performance Characteristics

Unless otherwise specified the following conditions apply:  $V_{IN} = 3.6V$ ,  $T_A = 25^\circ C$

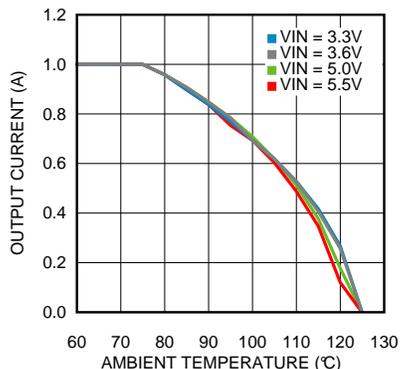
#### Dropout Voltage vs Load Current and Input Voltage



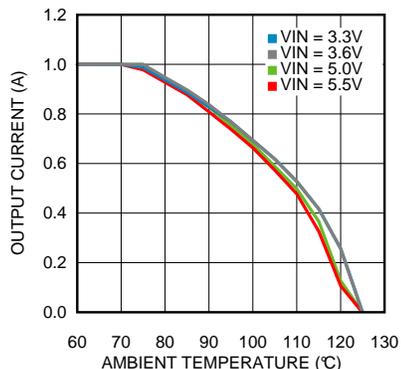
#### Thermal Derating $V_{OUT} = 1.2V$ , $\theta_{JA} = 120^\circ C/W$



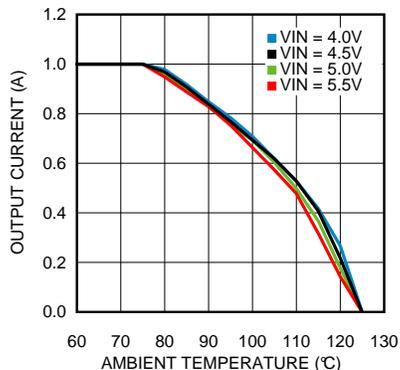
#### Thermal Derating $V_{OUT} = 1.8V$ , $\theta_{JA} = 120^\circ C/W$



#### Thermal Derating $V_{OUT} = 2.5V$ , $\theta_{JA} = 120^\circ C/W$

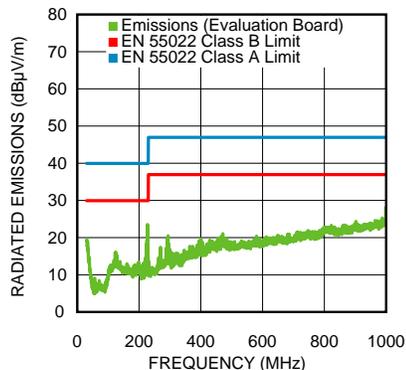


#### Thermal Derating $V_{OUT} = 3.3V$ , $\theta_{JA} = 120^\circ C/W$



#### Radiated EMI (CISPR22)

$V_{IN} = 5.0V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A$   
Default evaluation board BOM



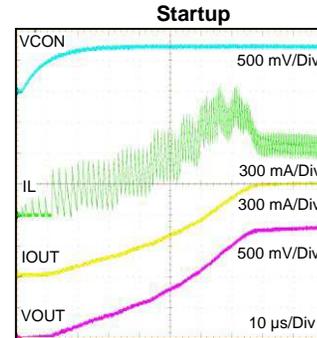
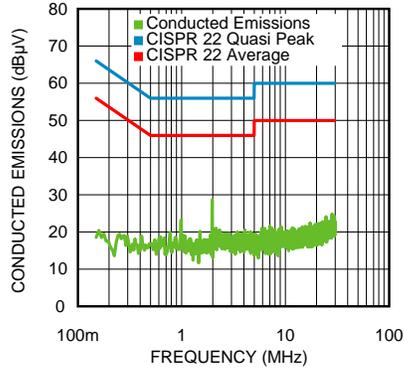
### Typical Performance Characteristics (continued)

Unless otherwise specified the following conditions apply:  $V_{IN} = 3.6V$ ,  $T_A = 25^\circ C$

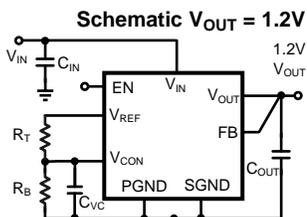
#### Conducted EMI

$V_{IN} = 5.0V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A$

Default evaluation board BOM with additional  $1\mu H$   $1\mu F$  LC input filter

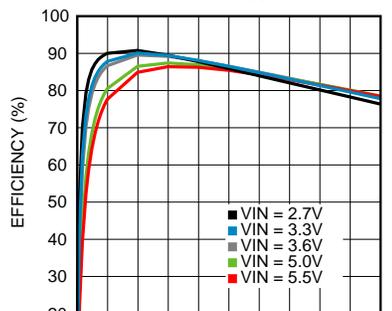


### 1.2V



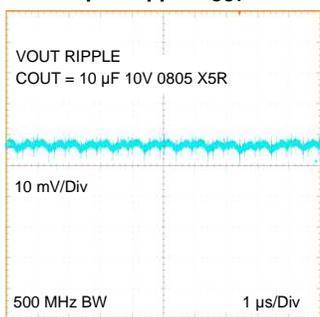
C <sub>IN</sub>	10 μF	≥ 6.3V	0805	X7R or X5R
C <sub>OUT</sub>	10 μF	≥ 6.3V	0805	X7R or X5R
C <sub>V<sub>C</sub></sub>	470 pF	≥ 6.3V	0603	X7R or X5R
R <sub>T</sub>	243 kΩ	1%	0603	
R <sub>B</sub>	63.4 kΩ	1%	0603	

Efficiency V<sub>OUT</sub> = 1.2V

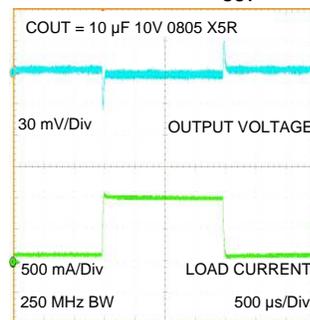


0.0 0.1 0.2 0.3 0.4 0.5 0.6 0.7 0.8 0.9 1.0  
LOAD CURRENT (A)

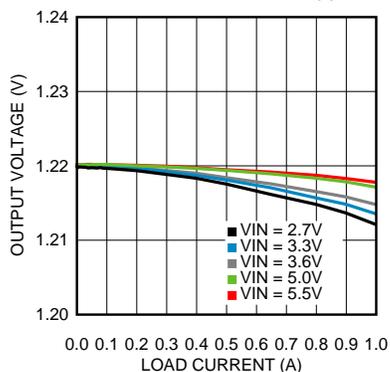
Output Ripple V<sub>OUT</sub> = 1.2V



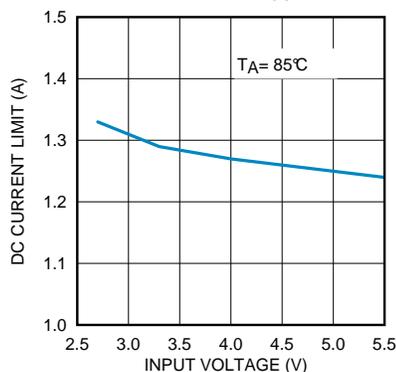
Load Transient V<sub>OUT</sub> = 1.2V



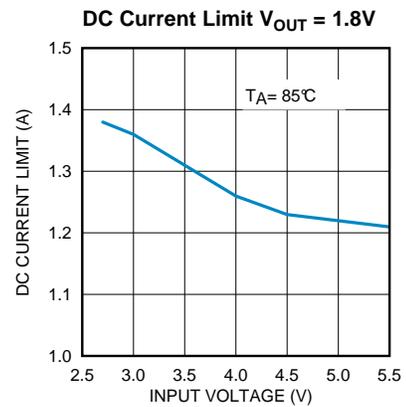
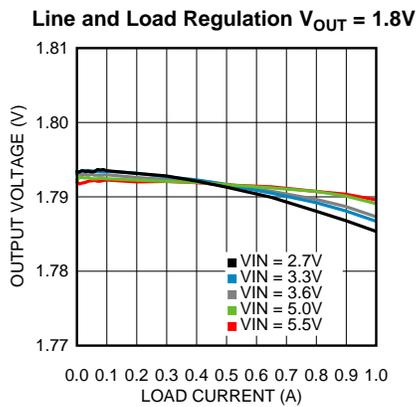
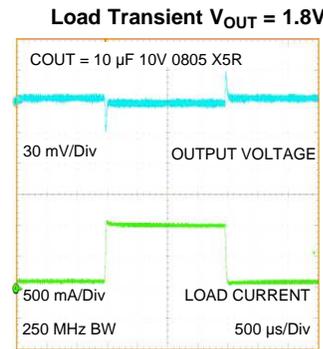
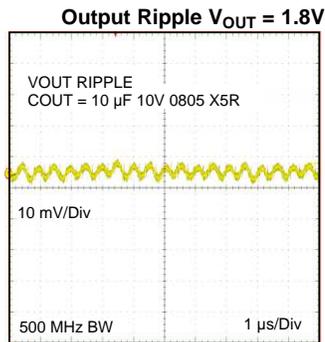
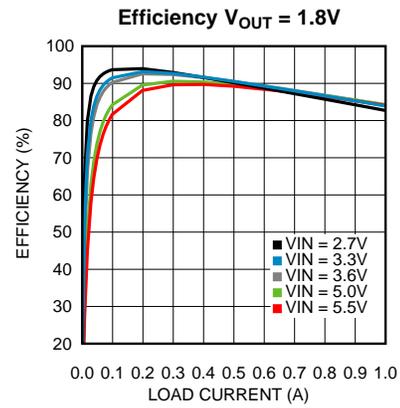
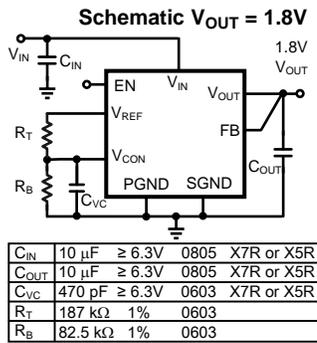
Line and Load Regulation V<sub>OUT</sub> = 1.2V



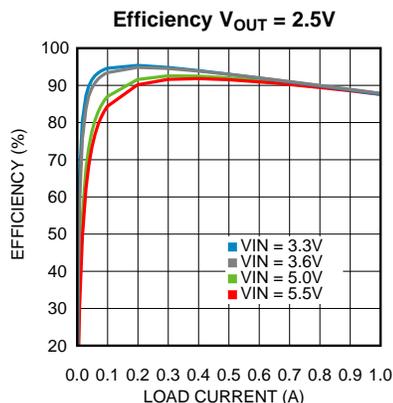
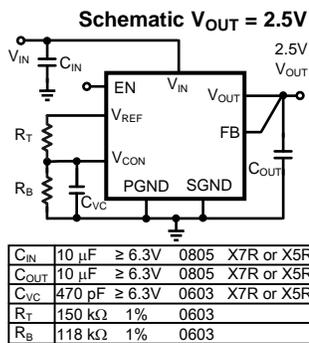
DC Current Limit V<sub>OUT</sub> = 1.2V



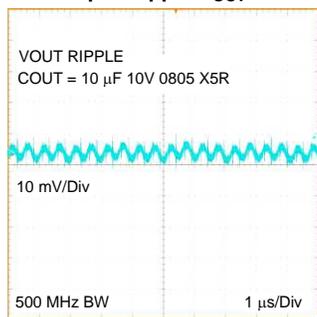
1.8V



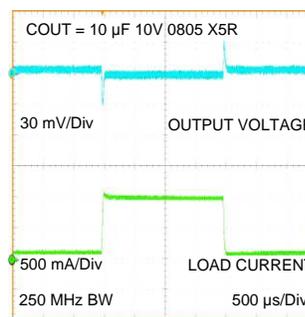
## 2.5V



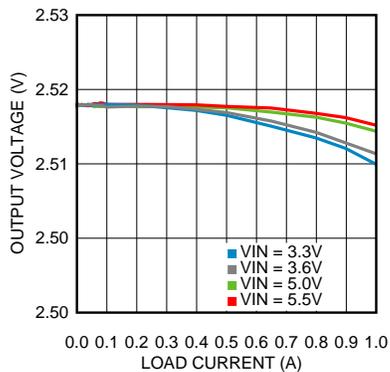
### Output Ripple $V_{OUT} = 2.5V$



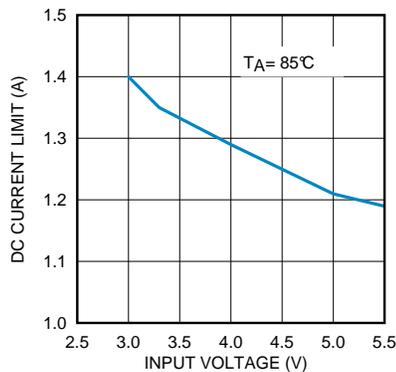
### Load Transient $V_{OUT} = 2.5V$



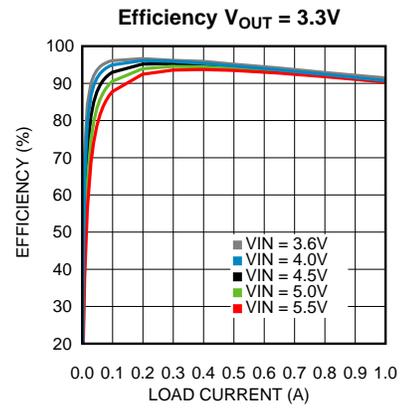
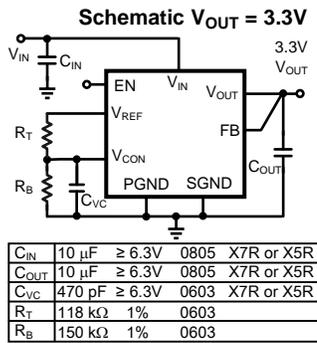
### Line and Load Regulation $V_{OUT} = 2.5V$



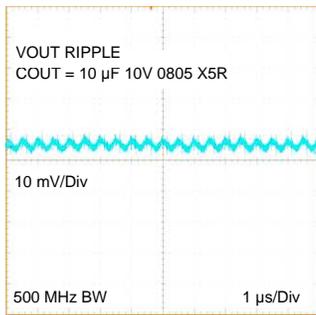
### DC Current Limit $V_{OUT} = 2.5V$



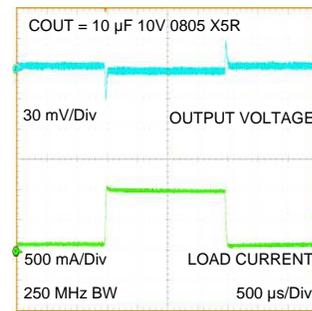
### 3.3V



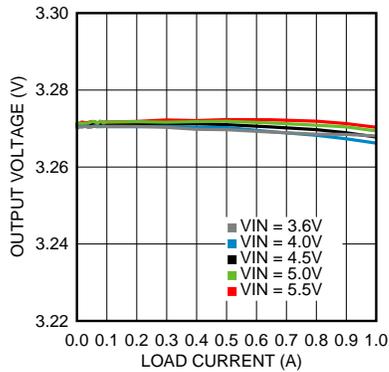
**Output Ripple  $V_{OUT} = 3.3V$**



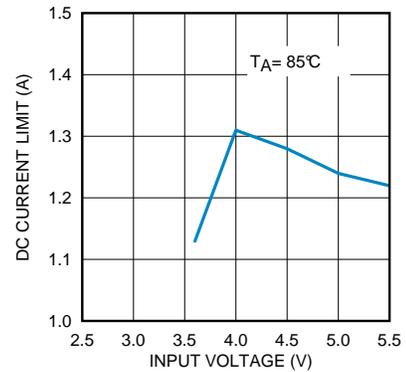
**Load Transient  $V_{OUT} = 3.3V$**



**Line and Load Regulation  $V_{OUT} = 3.3V$**



**DC Current Limit  $V_{OUT} = 3.3V$**



### BLOCK DIAGRAM

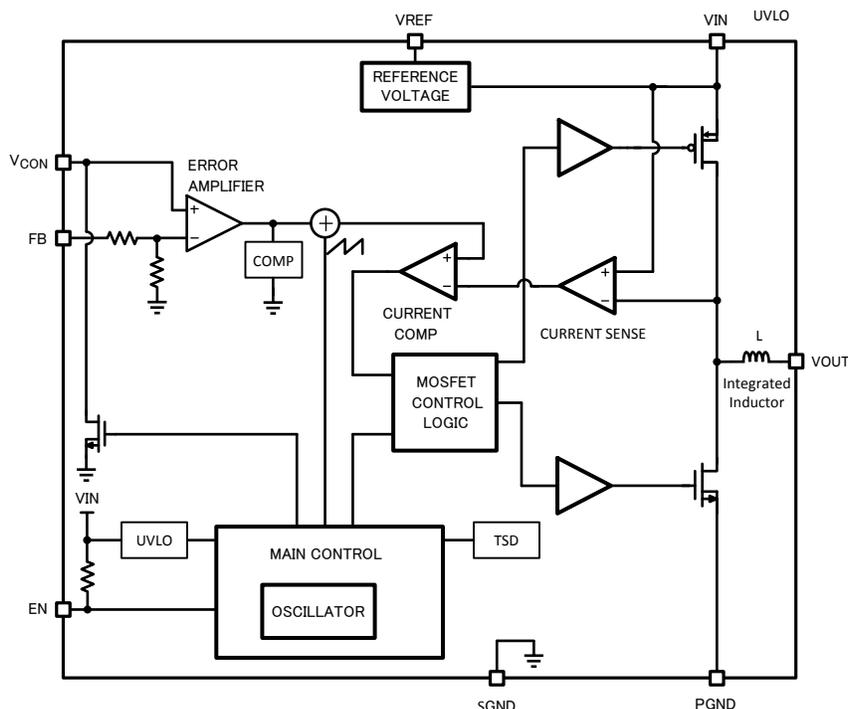


Figure 5. Functional Block Diagram

### Overview

The LMZ10501 SIMPLE SWITCHER® nano module is an easy-to-use step-down DC-DC solution capable of driving up to 1A load in space-constrained applications. Only an input capacitor, an output capacitor, a small  $V_{CON}$  filter capacitor, and two resistors are required for basic operation. The nano module comes in 8-pin LLP footprint package with an integrated inductor. The LMZ10501 operates in fixed 2.0MHz PWM (Pulse Width Modulation) mode, and is designed to deliver power at maximum efficiency. The output voltage is typically set by using a resistive divider between the built-in reference voltage  $V_{REF}$  and the control pin  $V_{CON}$ . The  $V_{CON}$  pin is the positive input to the error amplifier. The output voltage of the LMZ10501 can also be dynamically adjusted between 0.6V and 3.6V by driving the  $V_{CON}$  pin externally. Internal current limit based softstart function, current overload protection, and thermal shutdown are also provided.

### CIRCUIT OPERATION

The LMZ10501 is a synchronous Buck power module using a PFET for the high side switch and an NFET for the synchronous rectifier switch. The output voltage is regulated by modulating the PFET switch on-time. The circuit generates a duty-cycle modulated rectangular signal. The rectangular signal is averaged using a low pass filter formed by the integrated inductor and an output capacitor. The output voltage is equal to the average of the duty-cycle modulated rectangular signal. In PWM mode, the switching frequency is constant. The energy per cycle to the load is controlled by modulating the PFET on-time, which controls the peak inductor current. In current mode control architecture, the inductor current is compared with the slope compensated output of the error amplifier. At the rising edge of the clock, the PFET is turned ON, ramping up the inductor current with a slope of  $(V_{IN} - V_{OUT})/L$ . The PFET is ON until the current signal equals the error signal. Then the PFET is turned OFF and NFET is turned ON, ramping down the inductor current with a slope of  $V_{OUT}/L$ . At the next rising edge of the clock, the cycle repeats. An increase of load pulls the output voltage down, resulting in an increase of the error signal. As the error signal goes up, the peak inductor current is increased, elevating the average inductor current and responding to the heavier load. To ensure stability, a slope compensation ramp is subtracted from the error signal and internal loop compensation is provided.

## INPUT UNDER VOLTAGE DETECTION

The LMZ10501 implements an under voltage lock out (UVLO) circuit to ensure proper operation during startup, shutdown and input supply brownout conditions. The circuit monitors the voltage at the  $V_{IN}$  pin to ensure that sufficient voltage is present to bias the regulator. If the under voltage threshold is not met, all functions of the controller are disabled and the controller remains in a low power standby state.

## SHUTDOWN MODE

To shutdown the LMZ10501, pull the EN pin low ( $<0.5V$ ). In the shutdown mode all internal circuits are turned OFF.

## EN PIN OPERATION

The EN pin is internally pulled up to  $V_{IN}$  through a 790k $\Omega$  (typ.) resistor. This allows the nano module to be enabled by default when the EN pin is left floating. In such cases  $V_{IN}$  will set EN high when  $V_{IN}$  reaches 1.2V. As the input voltage continues to rise, operation will start once  $V_{IN}$  exceeds the under-voltage lockout (UVLO) threshold. To set EN high externally, pull it up to 1.2V or higher. Note that the voltage on EN must remain at less than  $V_{IN} + 0.2V$  due to absolute maximum ratings of the device.

## INTERNAL SYNCHRONOUS RECTIFICATION

The LMZ10501 uses an internal NFET as a synchronous rectifier to minimize the switch voltage drop and increase efficiency. The NFET is designed to conduct through its intrinsic body diode during the built-in dead time between the PFET on-time and the NFET on-time. This eliminates the need for an external diode. The dead time between the PFET and NFET connection prevents shoot through current from  $V_{IN}$  to PGND during the switching transitions.

## CURRENT LIMIT

The LMZ10501 current limit feature protects the module during an overload condition. The circuit employs positive peak current limit in the PFET and negative peak current limit in the NFET switch. The positive peak current through the PFET is limited to 1.7A (typ.). When the current reaches this limit threshold the PFET switch is immediately turned off until the next switching cycle. This behavior continues on a cycle-by-cycle basis until the overload condition is removed from the output. The typical negative peak current limit through the NFET switch is -0.6A (typ.).

The ripple of the inductor current depends on the input and output voltages. This means that the DC level of the output current when the peak current limiting occurs will also vary over the line voltage and the output voltage level. Refer to the DC Output Current Limit plots in the [Typical Performance Characteristics](#) section for more information.

## STARTUP BEHAVIOR AND SOFTSTART

The LMZ10501 features a current limit based soft start circuit in order to prevent large in-rush current and output overshoot as  $V_{OUT}$  is ramping up. This is achieved by gradually increasing the PFET current limit threshold to the final operating value as the output voltage ramps during startup. The maximum allowed current in the inductor is stepped up in a staircase profile for a fixed number of switching periods in each step. Additionally, the switching frequency in the first step is set at 450kHz and is then increased for each of the following steps until it reaches 2MHz at the final step of current limiting. This current limiting behavior is illustrated in [Figure 6](#) and allows for a smooth  $V_{OUT}$  ramp up.

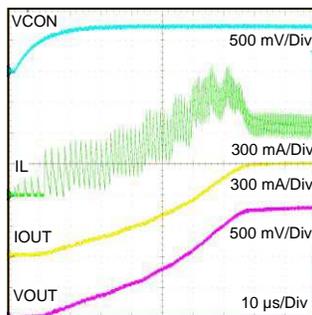


Figure 6. Startup behavior of current limit based softstart.

The soft start rate is also limited by the  $V_{CON}$  ramp up rate. The  $V_{CON}$  pin is discharged internally through a pull down device before startup occurs. This is done to deplete any residual charge on the  $V_{CON}$  filter capacitor and allow the  $V_{CON}$  voltage to ramp up from 0V when the part is started. The events that cause  $V_{CON}$  discharge are thermal shutdown, UVLO, EN low, or output short circuit detection. The minimum recommended capacitance on  $V_{CON}$  is 220pF and the maximum is 1nF. The duration of startup current limiting sequence takes approximately 75 $\mu$ s. After the sequence is completed, the feedback voltage is monitored for output short circuit events.

### OUTPUT SHORT CIRCUIT PROTECTION

In addition to cycle by cycle current limit, the LMZ10501 features a second level of short circuit protection. If the load pulls the output voltage down and the feedback voltage falls to 0.375V, the output short circuit protection will engage. In this mode the internal PFET switch is turned OFF after the current limit comparator trips and the beginning of the next cycle is inhibited for approximately 230 $\mu$ s. This forces the inductor current to ramp down and limits excessive current draw from the input supply when the output of the regulator is shorted. The synchronous rectifier is always OFF in this mode. After 230 $\mu$ s of non-switching a new startup sequence is initiated. During this new startup sequence the current limit is gradually stepped up to the nominal value as illustrated in the [STARTUP BEHAVIOR AND SOFTSTART](#) section. After the startup sequence is completed again, the feedback voltage is monitored for output short circuit. If the short circuit is still persistent after the new startup sequence, switching will be stopped again and there will be another 230 $\mu$ s off period. A persistent output short condition results in a hiccup behavior where the LMZ10501 goes through the normal startup sequence, then detects the output short at the end of startup, terminates switching for 230 $\mu$ s, and repeats this cycle until the output short is released. This behavior is illustrated in [Figure 7](#).

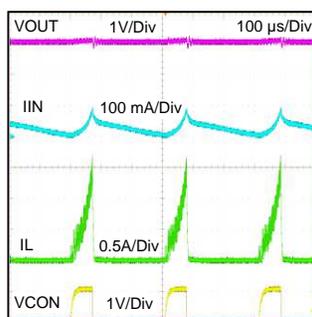
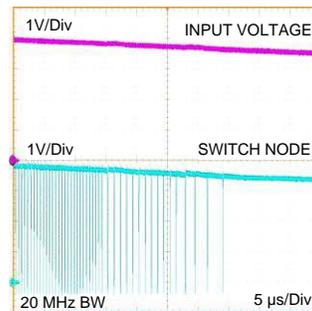


Figure 7. Hiccup behavior with persistent output short circuit.

Since the output current is limited during normal startup by the softstart function, the current charging the output capacitor is also limited. This results in a smooth  $V_{OUT}$  ramp up to nominal voltage. However, using excessively large output capacitance or  $V_{CON}$  capacitance under normal conditions can prevent the output voltage from reaching 0.375V at the end of the startup sequence. In such cases the module will maintain the described above hiccup mode and the output voltage will not ramp up to final value. To cause this condition, one would have to use unnecessarily large output capacitance for 1A load applications. See the [INPUT AND OUTPUT CAPACITOR SELECTION](#) section for guidance on maximum capacitances for different output voltage settings.

## HIGH DUTY CYCLE OPERATION

The LMZ10501 features a transition mode designed to extend the output regulation range to the minimum possible input voltage. As the input voltage decreases closer and closer to  $V_{OUT}$ , the off-time of the PFET gets smaller and smaller and the duty cycle eventually needs to reach 100% to support the output voltage. The input voltage at which the duty cycle reaches 100% is the edge of regulation. When the LMZ10501 input voltage is lowered, such that the off-time of the PFET reduces to less than 35ns, the LMZ10501 doubles the switching period to extend the off-time for that  $V_{IN}$  and maintain regulation. If  $V_{IN}$  is lowered even more, the off-time of the PFET will reach the 35ns mark again. The LMZ10501 will then reduce the frequency again, achieving less than 100% duty cycle operation and maintaining regulation. As  $V_{IN}$  is lowered even more, the LMZ10501 will continue to scale down the frequency, aiming to maintain at least 35ns off time. Eventually, as the input voltage decreases further, 100% duty cycle is reached. This behavior of extending the  $V_{IN}$  regulation range is illustrated in the following plot.



**Figure 8. High duty cycle operation and switching frequency reduction.**

## THERMAL OVERLOAD PROTECTION

The junction temperature of the LMZ10501 should not be allowed to exceed its maximum operating rating of 125°C. Thermal protection is implemented by an internal thermal shutdown circuit which activates at 150°C (typ). When this temperature is reached, the device enters a low power standby state. In this state switching remains off causing the output voltage to fall. Also, the  $V_{CON}$  capacitor is discharged to SGND. When the junction temperature falls back below 130 °C (typ) normal startup occurs and  $V_{OUT}$  rises smoothly from 0V. Applications requiring maximum output current may require derating at elevated ambient temperature. See the [Typical Performance Characteristics](#) section for thermal derating plots for various output voltages.

## APPLICATION INFORMATION

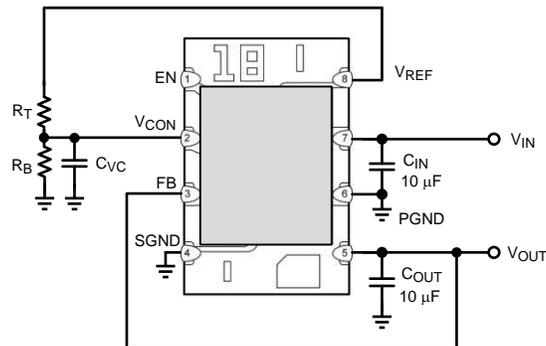


Figure 9. Typical Application Circuit

### SETTING THE OUTPUT VOLTAGE

The LMZ10501 provides a fixed 2.35V  $V_{REF}$  voltage output. As shown in Figure 9 above, a resistive divider formed by  $R_T$  and  $R_B$  sets the  $V_{CON}$  pin voltage level. The  $V_{OUT}$  voltage tracks  $V_{CON}$  and is governed by the following relationship:

$$V_{OUT} = GAIN \times V_{CON} \quad (1)$$

where GAIN is 2.5V/V from  $V_{CON}$  to  $V_{FB}$ .

This equation is valid for output voltages between 0.6V and 3.6V and corresponds to  $V_{CON}$  voltage between 0.24V and 1.44V, respectively.

#### $R_T$ and $R_B$ Selection for Fixed $V_{OUT}$

The parameters affecting the output voltage setting are the  $R_T$ ,  $R_B$ , and the product of the  $V_{REF}$  voltage x GAIN. The  $V_{REF}$  voltage is typically 2.35V. Since  $V_{CON}$  is derived from  $V_{REF}$  via  $R_T$  and  $R_B$ ,

$$V_{CON} = V_{REF} \times R_B / (R_B + R_T) \quad (2)$$

After substitution,

$$V_{OUT} = V_{REF} \times GAIN \times R_B / (R_B + R_T) \quad (3)$$

$$R_T = (GAIN \times V_{REF} / V_{OUT} - 1) \times R_B \quad (4)$$

The ideal product of  $GAIN \times V_{REF} = 5.875V$ .

Choose  $R_T$  to be between 80k $\Omega$  and 300k $\Omega$ . Then,  $R_B$  can be calculated using Equation 5 below.

$$R_B = (V_{OUT} / (5.875V - V_{OUT})) \times R_T \quad (5)$$

Note that the resistance of  $R_T$  should be  $\geq 80k\Omega$ . This ensures that the  $V_{REF}$  output current loading is not exceeded and the reference voltage is maintained. The current loading on  $V_{REF}$  should not be greater than 30  $\mu A$ .

### OUTPUT VOLTAGE ACCURACY OPTIMIZATION

Each nano module is optimized to achieve high  $V_{OUT}$  accuracy. Equation 1 shows that, by design, the output voltage is a function of the  $V_{CON}$  voltage and the gain from  $V_{CON}$  to  $V_{FB}$ . The voltage at  $V_{CON}$  is derived from  $V_{REF}$ . Therefore, as shown in Equation 3, the accuracy of the output voltage is a function of the  $V_{REF} \times GAIN$  product as well as the tolerance of the  $R_T$  and  $R_B$  resistors. The typical  $V_{REF} \times GAIN$  product by design is 5.875V. Each nano module's  $V_{REF}$  voltage is trimmed so that this product is as close to the ideal 5.875V value as possible, achieving high  $V_{OUT}$  accuracy. See the Electrical Specifications section for the  $V_{REF} \times GAIN$  product tolerance limits.

## DYNAMIC OUTPUT VOLTAGE SCALING

The  $V_{CON}$  pin on the LMZ10501 can be driven externally by a DAC to scale the output voltage dynamically. The output voltage  $V_{OUT} = 2.5V/V \times V_{CON}$ . When driving  $V_{CON}$  with a source different than  $V_{REF}$  place a 1.5k $\Omega$  resistor in series with the  $V_{CON}$  pin. Current limiting the external  $V_{CON}$  helps to protect this pin and allows the  $V_{CON}$  capacitor to be fully discharged to 0V after fault conditions.

## INTEGRATED INDUCTOR

The LMZ10501 uses a Low Temperature Co-fired Ceramic (LTCC) type 2.6  $\mu$ H inductor with over 1.2A DC current rating and soft saturation profile for up to 2A. This inductor allows for the 1.425mm maximum package height providing an easy to use, compact solution with reduced EMI.

## INPUT AND OUTPUT CAPACITOR SELECTION

The LMZ10501 is designed for use with low ESR multi-layer ceramic capacitors (MLCC) for its input and output filters. Using a 10  $\mu$ F 0603 or 0805 with 6.3V or 10V rating ceramic input capacitor typically provides sufficient  $V_{IN}$  bypass. Use of multiple 4.7  $\mu$ F or 2.2 $\mu$ F capacitors can also be considered. Ceramic capacitors with X5R and X7R temperature characteristics are recommended for both input and output filters. These provide an optimal balance between small size, cost, reliability, and performance for space sensitive applications.

The DC voltage bias characteristics of the capacitors must be considered when selecting the DC voltage rating and case size of these components. The effective capacitance of an MLCC is typically reduced by the DC voltage bias applied across its terminals. For example, a typical 0805 case size X5R 6.3V 10  $\mu$ F ceramic capacitor may only have 4.8  $\mu$ F left in it when a 5.0V DC bias is applied. Similarly, a typical 0603 case size X5R 6.3V 10  $\mu$ F ceramic capacitor may only have 2.4  $\mu$ F at the same 5.0V DC. Smaller case size capacitors may have even larger percentage drop in value with DC bias.

The optimum output capacitance value is application dependent. Too small output capacitance can lead to instability due to lower loop phase margin. On the other hand, if the output capacitor is too large, it may prevent the output voltage from reaching the 0.375V required voltage level at the end of the startup sequence. In such cases, the output short circuit protection can be engaged and the nano module will enter a hiccup mode as described in the [OUTPUT SHORT CIRCUIT PROTECTION](#) section. [Table 2](#) sets the minimum output capacitance for stability and maximum output capacitance for proper startup for various output voltage settings. Note that the maximum  $C_{OUT}$  value in [Table 2](#) assumes that the filter capacitance on  $V_{CON}$  is the maximum recommended value of 1nF and the  $R_T$  resistor value is less than 300k $\Omega$ . Lower  $V_{CON}$  capacitance can extend the maximum  $C_{OUT}$  range. There is no great performance benefit in using excessive  $C_{OUT}$  values.

**Table 2. Output Capacitance Range**

Output Voltage	Minimum $C_{OUT}$	Suggested $C_{OUT}$	Maximum $C_{OUT}$
0.6V	4.7 $\mu$ F	10 $\mu$ F	47 $\mu$ F
1.0V	3.3 $\mu$ F	10 $\mu$ F	47 $\mu$ F
1.2V	3.3 $\mu$ F	10 $\mu$ F	47 $\mu$ F
1.8V	3.3 $\mu$ F	10 $\mu$ F	68 $\mu$ F
2.5V	3.3 $\mu$ F	10 $\mu$ F	100 $\mu$ F
3.3V	3.3 $\mu$ F	10 $\mu$ F	100 $\mu$ F

Use of multiple 4.7  $\mu$ F or 2.2 $\mu$ F output capacitors can be considered for reduced effective ESR and smaller output voltage ripple. In addition to the main output capacitor, small 0.1 $\mu$ F – 0.01 $\mu$ F parallel capacitors can be used to reduce high frequency noise.

## PACKAGE CONSIDERATIONS

The nano module package includes an LTCC inductor on the bottom and a micro SMD die mounted on top. The die has exposed edges and can be sensitive to ambient light. For applications with direct high intensity ambient red, infrared, LED, or natural light it is recommended to have the device shielded from the light source to avoid abnormal behavior.

Since the die is exposed on top of the package, care should be taken when picking and placing the module on the board.

Use the following recommendations when utilizing machine placement:

- Use 1.06mm (42mil) or smaller nozzle size so that the nozzle head does not touch the outer area of the exposed die.
- Use a soft tip pick and place head.
- Add 0.05mm to the component thickness so that the device will be released 0.05mm (2mil) into the solder paste without putting pressure or splashing the solder paste.
- Slow the pick arm when picking the part from the tape and reel carrier and when depositing the IC on the board.
- If the machine releases the component by force, use minimum force or no more than 3 Newtons.
- For PCBs with surface mount components on both sides, it is suggested to put the LMZ10501 on the top side. In case the application requires bottom side placement, a reflow fixture may be required to protect the module during the second reflow.

For manual placement:

- Use a vacuum pick up hand tool with soft tip head.
- If vacuum pick up tool is not available, use non-metal tweezers and hold the part by the inductor body side terminals rather than the micro SMD die on top.
- Use minimal force when picking and placing the module on the board.
- In case a heat gun is required for rework, make sure that the heat source is pointing at the interface between the inductor and the PCB. Do not apply heat gun directly on top of the component since it may affect the solder joint between the micro SMD and the inductor. Using hot air station provides better temperature control and better controlled air flow than a heat gun.
- Go to the video section at [www.ti.com/product/lmz10501](http://www.ti.com/product/lmz10501) for a quick video on how to solder rework the LMZ10501.

### Board Layout Considerations

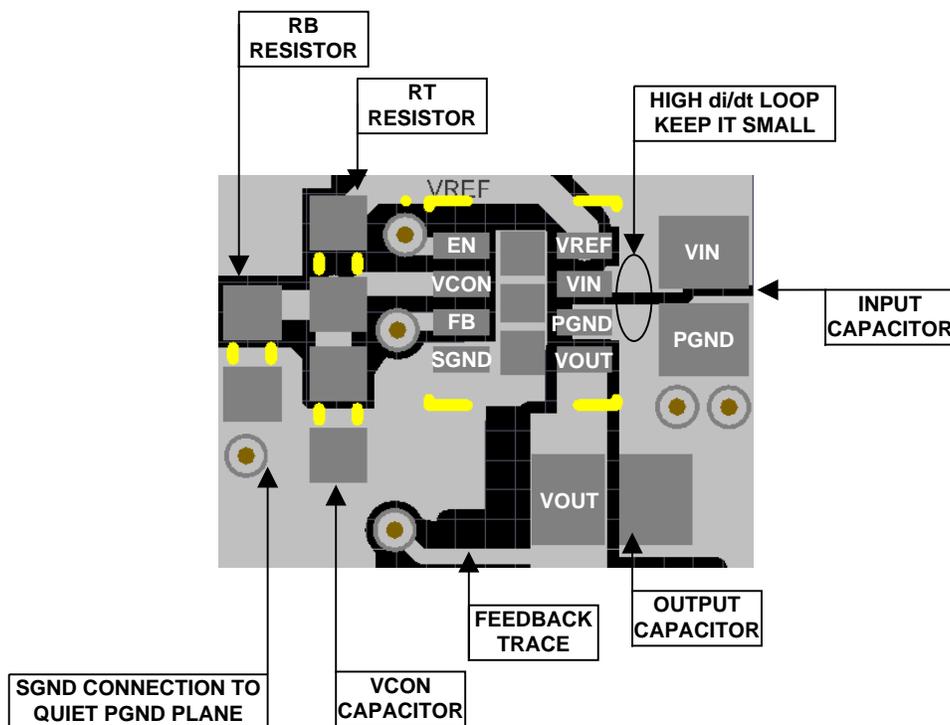


Figure 10. Example Top Layer Board Layout

The board layout of any DC-DC switching converter is critical for the optimal performance of the design. Bad PCB layout design can disrupt the operation of an otherwise good schematic design. Even if the regulator still converts the voltage properly, the board layout can mean the difference between passing or failing EMI regulations. In a Buck converter, the most critical board layout path is between the input capacitor ground terminal and the synchronous rectifier ground. The loop formed by the input capacitor and the power FETs is a path for the high  $di/dt$  switching current during each switching period. This loop should always be kept as short as possible when laying out a board for any Buck converter.

The LMZ10501 integrates the inductor and simplifies the DC-DC converter board layout. Refer to the example layout in [Figure 10](#). There are a few basic requirements to achieve a good LMZ10501 layout.

- 1. Place the input capacitor  $C_{IN}$  as close as possible to the  $V_{IN}$  and PGND terminals.**  $V_{IN}$  (pin 7) and PGND (pin 6) on the LMZ10501 are next to each other which makes the input capacitor placement simple.
- 2. Place the  $V_{CON}$  filter capacitor  $C_{VC}$  and the  $R_B$   $R_T$  resistive divider as close as possible to the  $V_{CON}$  and SGND terminals.** The  $C_{VC}$  capacitor (not  $R_B$ ) should be the component closer to the  $V_{CON}$  pin, as shown in [Figure 10](#). This allows for better bypass of the control voltage set at  $V_{CON}$ .
- 3. Run the feedback trace (from  $V_{OUT}$  to FB) away from noise sources.**
- 4. Connect SGND to a quiet GND plane.**
- 5. Provide enough PCB area for proper heatsinking.** Refer to the [Electrical Characteristics](#) table for example  $\theta_{JA}$  values for different board areas. Also, refer to AN-2020 for additional thermal design hints.

Refer to the evaluation board application note AN-2166 for a complete board layout example.

**PACKAGING INFORMATION**

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish	MSL Peak Temp (3)	Samples (Requires Login)
LMZ10501SE/NOPB	ACTIVE	POS	NQA	8		TBD	Call TI	Call TI	
LMZ10501SEE/NOPB	ACTIVE	POS	NQA	8		TBD	Call TI	Call TI	
LMZ10501SEX/NOPB	ACTIVE	POS	NQA	8		TBD	Call TI	Call TI	
LMZ10501SH/NOPB	ACTIVE	POS	NQB	8	1000	Pb-Free (RoHS Exempt)	SNAGCU	Level-3-260C-168 HR	
LMZ10501SHE/NOPB	ACTIVE	POS	NQB	8	250	Pb-Free (RoHS Exempt)	Call TI	Level-3-260C-168 HR	
LMZ10501SHX/NOPB	ACTIVE	POS	NQB	8	3000	Pb-Free (RoHS Exempt)	Call TI	Level-3-260C-168 HR	

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBSOLETE:** TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

**TBD:** The Pb-Free/Green conversion plan has not been defined.

**Pb-Free (RoHS):** TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

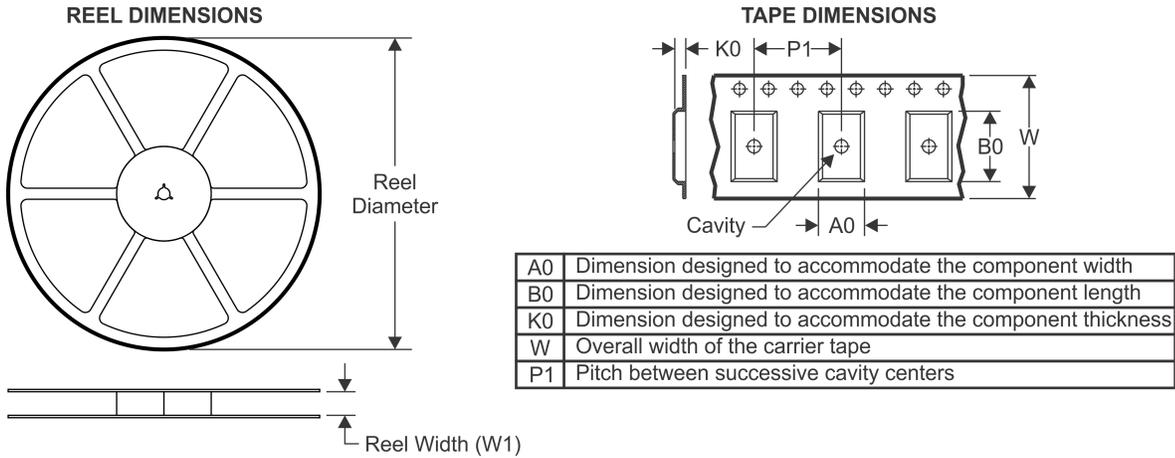
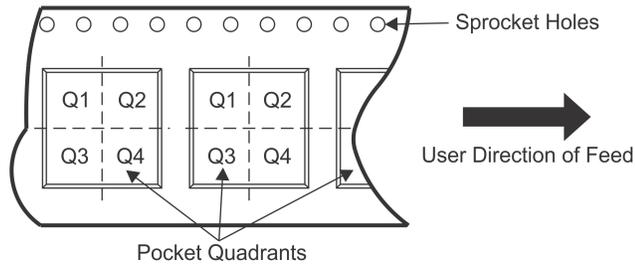
**Pb-Free (RoHS Exempt):** This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

**Green (RoHS & no Sb/Br):** TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. -- The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

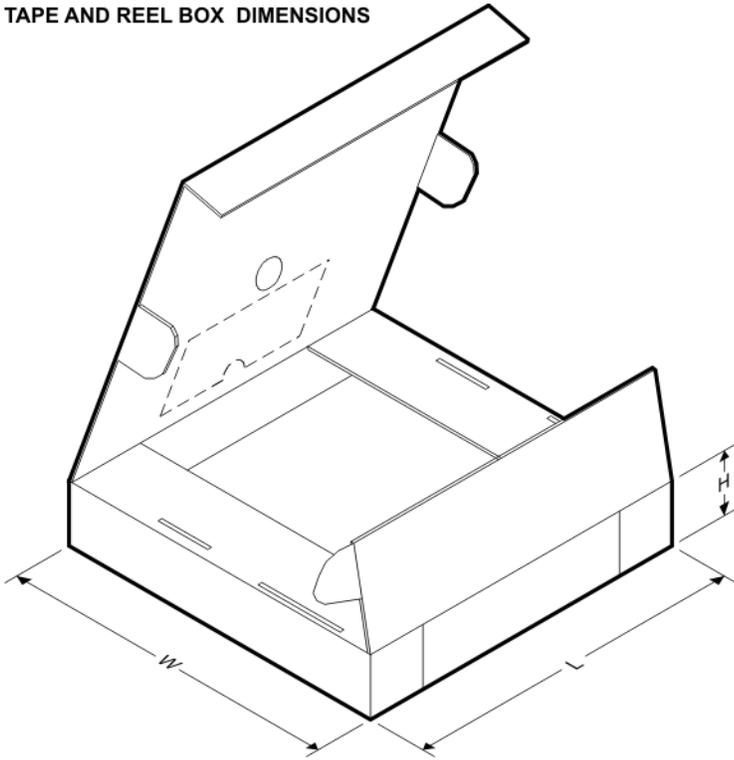
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**QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE**


\*All dimensions are nominal

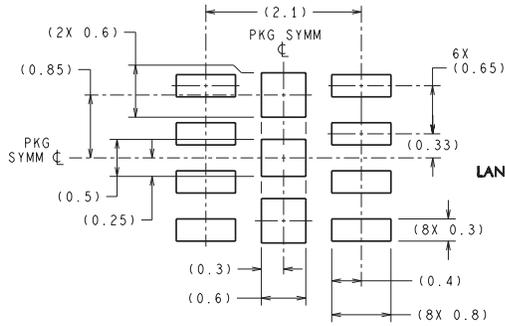
Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LMZ10501SHE/NOPB	POS	NQB	8	250	178.0	12.4	3.8	3.8	2.2	8.0	12.0	Q1
LMZ10501SHX/NOPB	POS	NQB	8	3000	330.0	12.4	3.8	3.8	2.2	8.0	12.0	Q1

**TAPE AND REEL BOX DIMENSIONS**


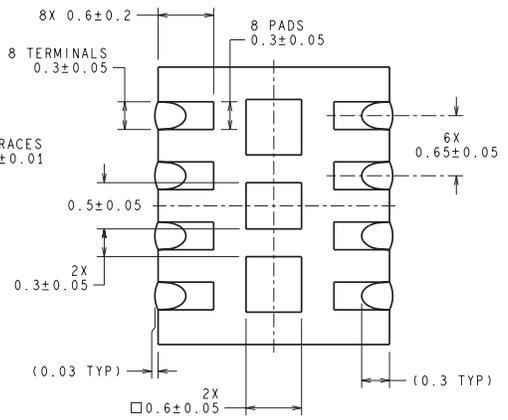
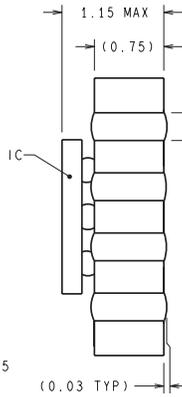
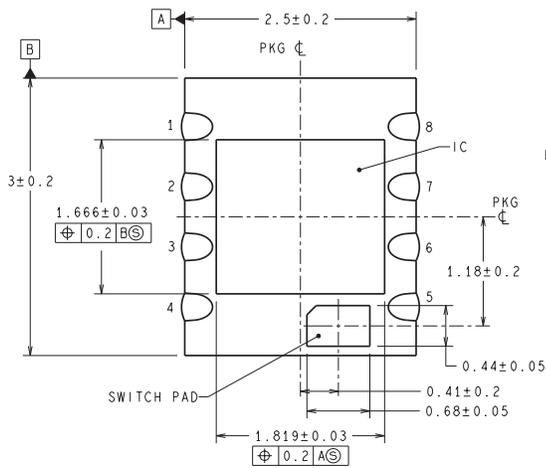
\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LMZ10501SHE/NOPB	POS	NQB	8	250	203.0	190.0	41.0
LMZ10501SHX/NOPB	POS	NQB	8	3000	358.0	343.0	63.0

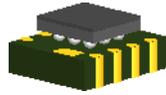
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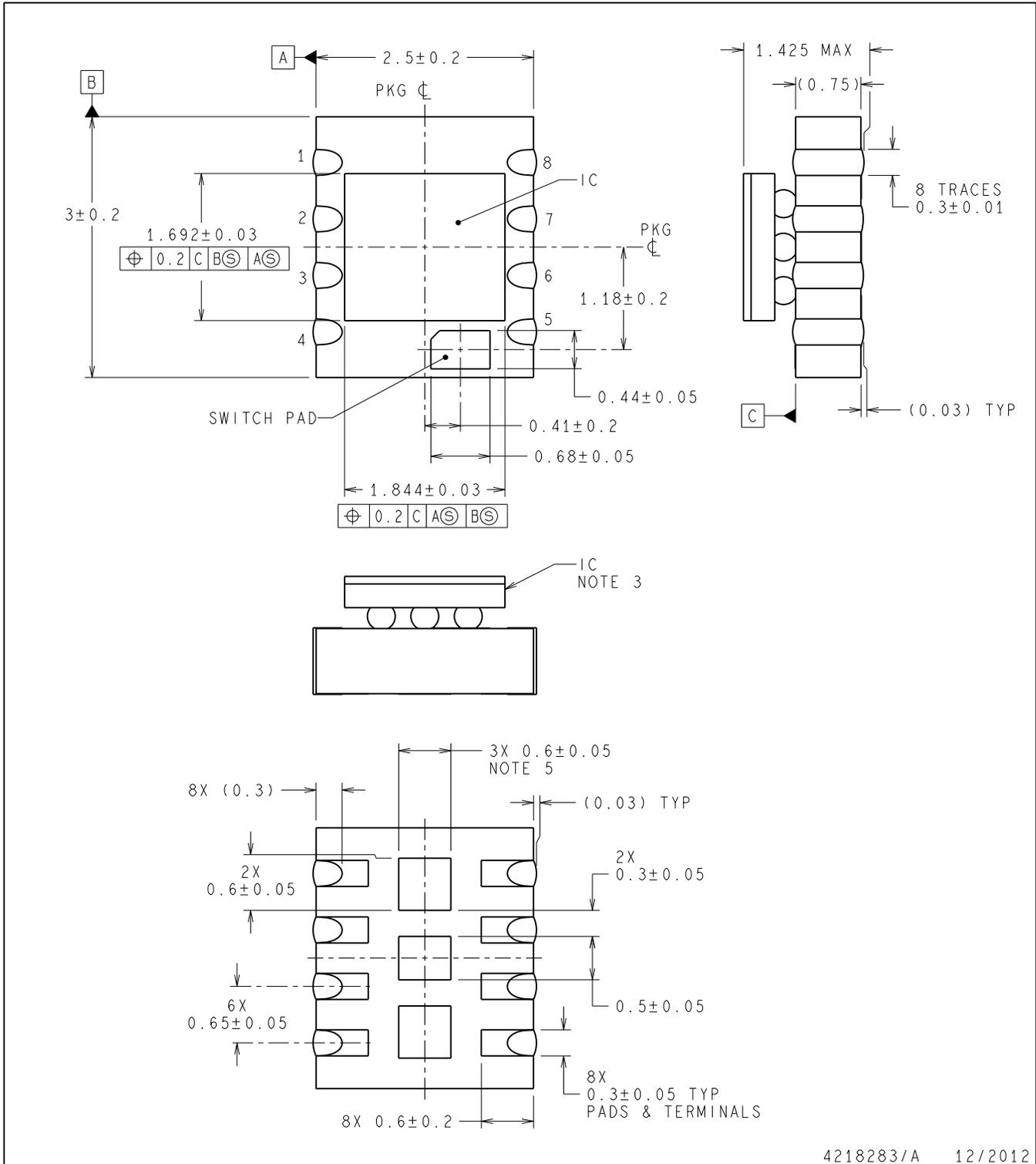
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**NQB0008A**

**POS - 1.425 mm max pkg height**

POS



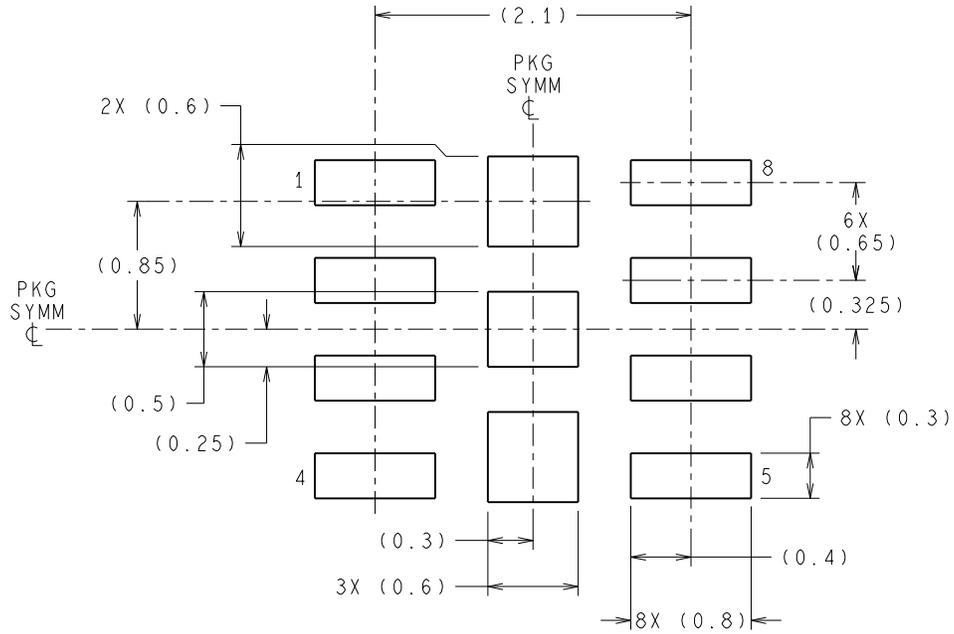
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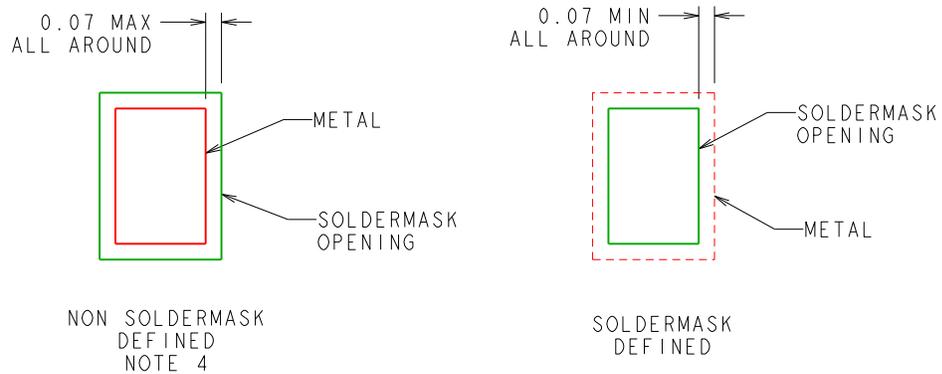
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POS - 1.425 mm max pkg height

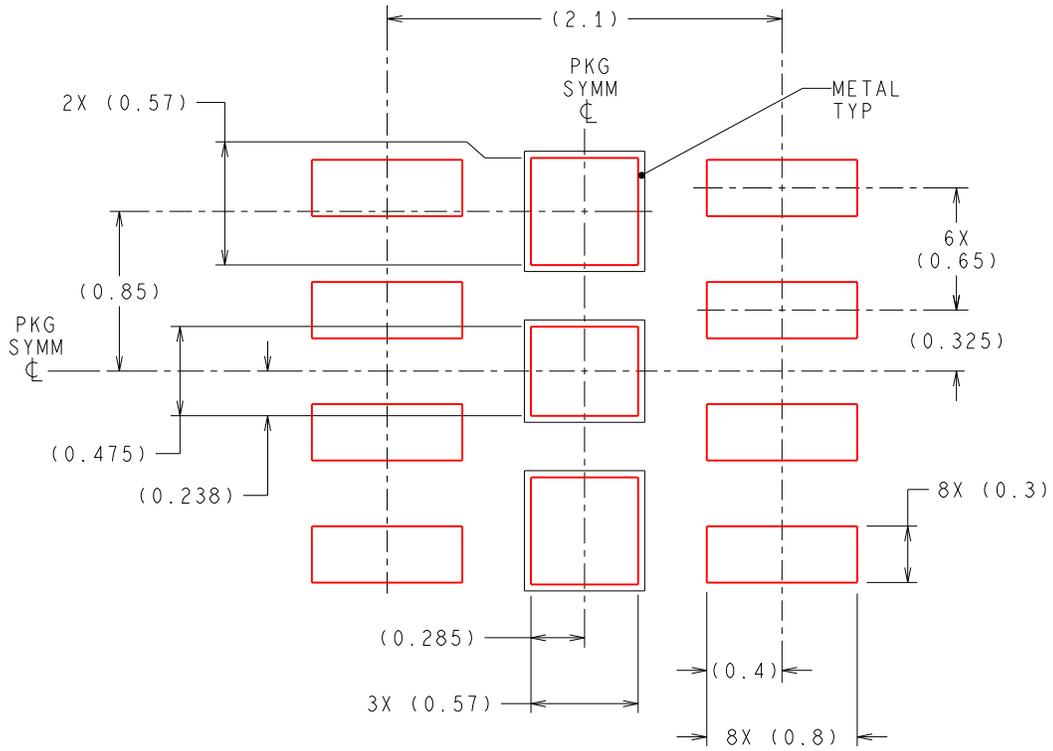
POS



RECOMMENDED LAND PATTERN



SOLDERMASK DETAILS  
NOT TO SCALE



**RECOMMENDED SOLDERPASTE**  
 CENTER ANCHOR PADS  
 90% PRINTED SOLDER COVERAGE BY AREA

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